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# **FPGA Design Automation: A Survey**

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### Abstract

Design automation or computer-aided design (CAD) for field programmable gate arrays (FPGAs) has played a critical role in the rapid advancement and adoption of FPGA technology over the past two decades. The purpose of this paper is to meet the demand for an up-to-date comprehensive survey/tutorial for FPGA design automation, with an emphasis on the recent developments within the past 5–10 years. The paper focuses on the theory and techniques that have been, or most likely will be, reduced to practice. It covers all major steps in FPGA design flow which includes: routing and placement, circuit clustering, technology mapping and architecture-specific optimization, physical synthesis, RT-level and behavior-level synthesis, and power optimization. We hope that this paper can be used both as a guide for beginners who are embarking on research in this relatively young yet exciting area, and a useful reference for established researchers in this field.

**Keywords:** computer-aided design; FPGA design

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# 1

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## Introduction

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The semiconductor industry has showcased the spectacular exponential growth of device complexity and performance for four decades, predicted by Moore’s Law. Programmable logic devices (PLDs), especially field programmable gate arrays (FPGAs), have also experienced an exponential growth in the past 20 years, in fact, at an even faster pace compared to the rest of the semiconductor industry. For example, when FPGAs were first debuted in the mid- to late-80s, the Xilinx XC2064 FPGA had only 64 lookup tables (LUTs) and it was used as simple glue logic. Now, both Altera’s Stratix II [10] and Xilinx’s Virtex-4 chips [205] offer up to over 200,000 programmable logic cells (i.e., LUTs), plus a large number of hard-wired macro blocks such as embedded memories, DSP blocks, embedded processors, high-speed IOs, and clock synchronization circuitry, representing an over 3,000 times increase in logic capacity. These FPGA devices are being used to implement highly complex system-on-a-chip (SoC) designs. To support the design of such complex programmable devices, computer-aided design (CAD) plays a critical role in delivering high-performance, high-density, and low-power design solutions using these high-end FPGAs. We witnessed the

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establishment of FPGA design automation as a research area and a dramatic increase in research activities in this area in the past 17–18 years. However, there is lack of comprehensive references for the latest FPGA CAD research. Most existing books (e.g., [23, 27, 92, 150, 186]) and survey/tutorial papers (e.g., [28, 52]) in this area are 10–15 years old, and do not reflect vast amount of recent research on FPGA CAD. The purpose of this paper is to meet the demand for a comprehensive survey/tutorial on the state of FPGA CAD—with an emphasis on the recent developments that have taken place within the past 5–10 years and a focus on the theory and techniques that have been, or most likely will be, reduced to practice. We hope that this paper can be useful for both beginners and established researchers in this exciting and dynamic field.

In the remainder of this section we shall first briefly introduce some typical FPGA architectures and define the basic terminologies that will be used in the rest of this paper. Then, we shall provide an overview of the FPGA design flow.

### 1.1 Introduction to FPGA Architectures

An FPGA chip includes input/output (I/O) blocks and the core programmable fabric. The I/O blocks are located around the periphery of the chip, providing programmable I/O connections and support for various I/O standards. The core programmable fabric consists of programmable logic blocks and programmable routing architectures. Figure 1.1 shows a high-level view of an island-style FPGA [23], which represents a popular architecture framework that many commercial FPGAs are based on, and is also a widely accepted architecture model used in the FPGA research community. *Logic blocks* represented by gray squares consist of circuitry for implementing logic. Logic blocks are also called configurable logic blocks (CLBs). Each logic block is surrounded by routing channels connected through switch blocks and connection blocks. The wires in the channels are typically segmented and the length of each wire segment can vary. A *switch block* connects wires in adjacent channels through programmable switches such as pass-transistors or bi-directional buffers. A *connection block* connects

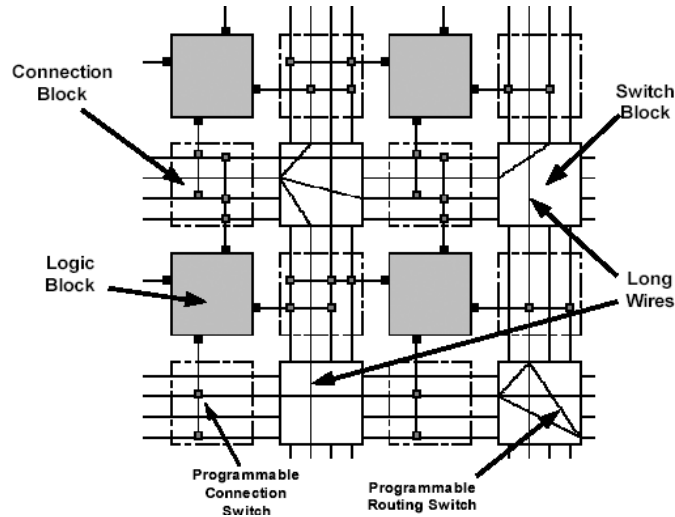


Fig. 1.1 An island-style FPGA [23].

the wire segments around a logic block to its inputs and outputs, also through programmable switches. Notice that the structures of the switch blocks are all identical. The figure illustrates the different switching and connecting situations in the switch blocks (the structures of all the connection blocks are identical as well). In [23] routing architectures are defined by the parameters of channel width ( $W$ ), switch block flexibility ( $F_s$  – the number of wires to which each incoming wire can connect in a switch block), connection block flexibility ( $F_c$  – the number of wires in each channel to which a logic block input or output pin can connect), and segmented wire lengths (the number of logic blocks a wire segment spans). Modern FPGAs also provide embedded IP cores, such as memories, DSP blocks, and processors, to facilitate the implementation of SoC designs.

Commercial FPGA chips contain a large amount of dedicated interconnects with different fixed lengths. These interconnects are usually point-to-point and uni-directional connections for performance improvement. For example, Altera’s Stratix II chip [10] has vertical or horizontal interconnects across 4, 16 or 24 logic blocks. There are dedicated carry chain and register chain interconnects within and between

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logic blocks as well. Xilinx’s Spartan-3E chip [204] has long lines, hex lines, double lines, and direct connections between the logic blocks. These lines cross different numbers of logic blocks. Specifically, the direct connect lines can route signals to neighboring tiles vertically, horizontally, and diagonally. For example, Figure 1.2 shows the direct connect lines (a) and hex lines (b) between a CLB and its neighbors in the Spartan-3E chip. The use of segmented routing makes the FPGA interconnect delays highly non-linear, discrete, and in some cases, even non-monotone (with respect to the distance). This presents unique challenges for FPGA placement and routing tools because a simple interconnect delay model using Manhattan distance between the source and the sink may not work well any more. Accurate interconnect delay modeling is a mandate for meaningful performance-driven physical design tools for FPGAs.

Further down the logic hierarchy, each logic block contains a group of basic logic elements (BLEs), where each BLE contains a

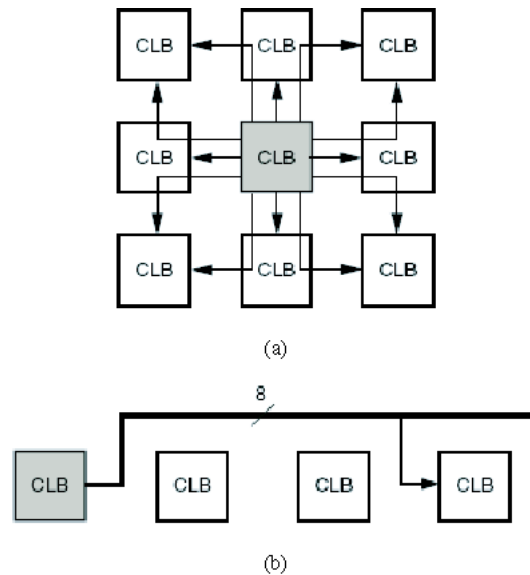


Fig. 1.2 Direct connect lines (a) and hex lines (b) in Xilinx Spartan-3E architecture [204].

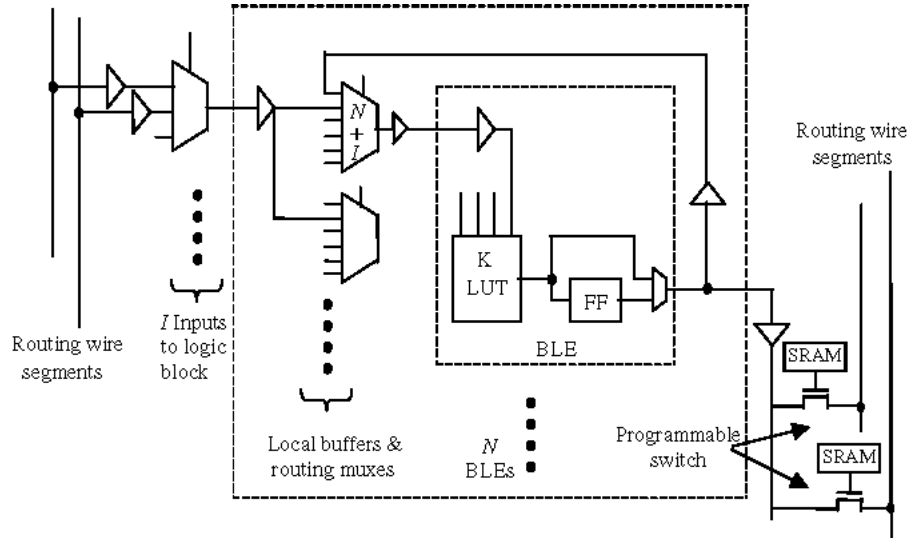


Fig. 1.3 A logic block and its peripheries.

LUT<sup>1</sup> and a register. Figure 1.3 shows part of a logic block with a block size  $N$  (the logic block contains  $N$  BLEs). The logic block has  $I$  inputs and  $N$  outputs. These inputs and outputs are fully connected to the inputs of each LUT through multiplexers. The figure also shows some details of the peripheral circuitry in the routing channels.

In addition to logic and routing architectures, clock distribution networks is another important aspect of FPGA chips. An H-tree based FPGA clock network is shown in Fig. 1.4 [130]. A tile is a logic block. Each clock tree buffer in the H-tree has two branches. There is a local clock buffer for each flip-flop in a tile. Both clock tree buffers in the H-tree and local clock buffers in the tiles are considered to be clock network resources. Chip area, tile size, and channel width determine the depth of the clock tree and the lengths of the tree branches.

<sup>1</sup> We focus on the LUT-based FPGA architecture in which the BLE consists of one  $k$ -input lookup table ( $k$ -LUT) and one flip-flop. The output of the  $k$ -LUT can be either registered or un-registered. We want to point out that commercial FPGAs may use slightly different logic architectures. For example, Altera’s Stratix II FPGA [10] uses an adaptive logic module which contains a group of LUTs and a pair of flip-flops.

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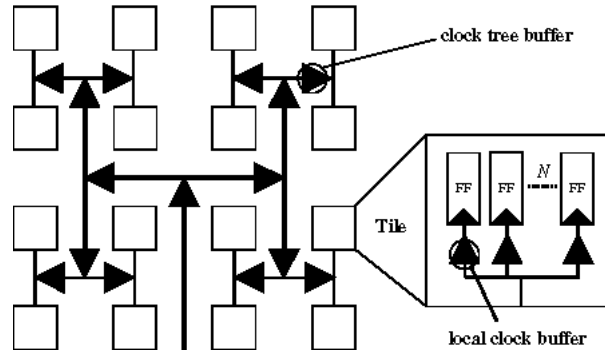


Fig. 1.4 A clock tree [130].

There is another type of programmable logic device called complex programmable logic device (CPLD). The general architecture topology of a CPLD chip is similar to that of island-based FPGAs, where routing resources surround logic blocks. One attribute of CPLD is that its interconnected structures are simpler than those of FPGAs. Therefore, the interconnect delay of CPLD is more predictable compared to that of FPGAs. The basic logic elements in the CPLD logic blocks are not LUTs. Instead, they are logic cells based on two-level AND-OR structures, where a fixed number of AND gates (also called p-terms) drive an OR gate. The output from the OR gate can be registered as well. For example, Fig. 1.5 shows such a structure (called *macrocell*) used in Altera’s MAX7000B CPLD [6]. Each macrocell has five p-terms by default. It can borrow some p-terms from its neighbors. The interconnect structure PIA (programmable interconnect array) connects different logic blocks together.

## 1.2 Overview of FPGA Design Flow

As the FPGA architecture evolves and its complexity increases, CAD software has become more mature as well. Today, most FPGA vendors provide a fairly complete set of design tools that allows automatic synthesis and compilation from design specifications in hardware specification languages, such as Verilog or VHDL, all the way down

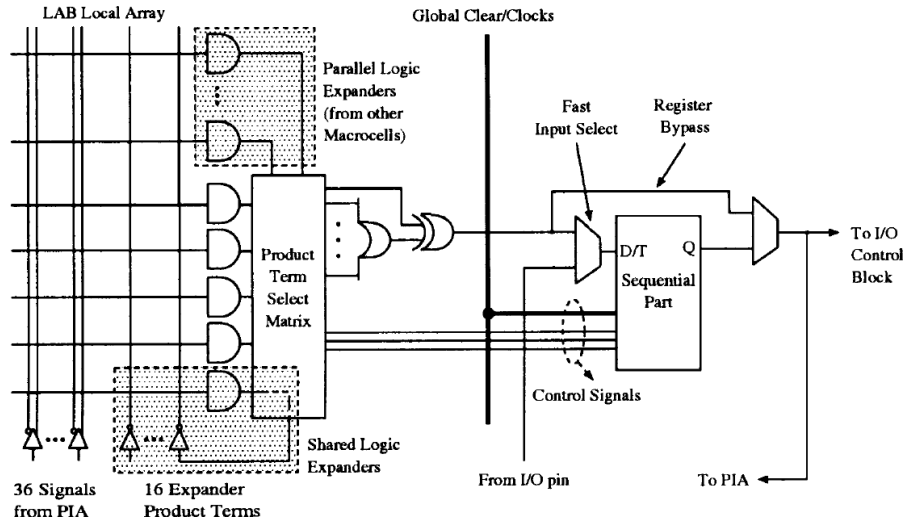


Fig. 1.5 An example of CPLD logic element, MAX 7000B macrocell [6].

to a bit-stream to program FPGA chips. A typical FPGA design flow includes the steps and components shown in Fig. 1.6.

Inputs to the design flow typically include the HDL specification of the design, design constraints, and specification of target FPGA devices. We further elaborate on these components of the design input in the following:

- The most widely used design specification languages are Verilog and VHDL at the register transfer level (RTL) which specify the operations at each clock cycle. There is a general (although rather slow) trend toward moving to specification at a higher level of abstraction, using general-purpose behavior description languages like C or SystemC [180], or domain-specific languages, such as MatLab [183] or Simulink [183]. Using these languages, one can specify the behavior of the design without going through a cycle-accurate detailed description of the design. A behavior synthesis tool is used to generate the RTL specification in Verilog or VHDL, which is then fed into the design flow as shown in Fig. 1.6. We shall discuss the behavior synthesis techniques in Section 5.

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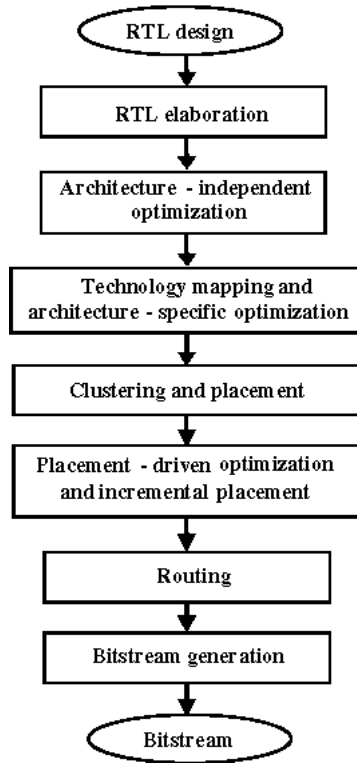


Fig. 1.6 A typical FPGA design flow starting from RTL specifications.

- Design constraints typically include the expected operating frequencies of different clocks, the delay bounds of the signal path delays from input pads to output pads (I/O delay), from the input pads to registers (setup time), and from registers to output pads (clock-to-output delay). In some cases, delays between some specific pairs of registers may be constrained. Design constraints may also include specifications of so-called *false paths* and *multi-cycle paths*. False paths will not be activated during normal circuit operation, and therefore can be ignored; multi-cycle paths refer to signal paths that carry a valid signal every few clock cycles, and therefore have a relaxed timing requirement. Typically, the designer



specifies the false paths and multi-cycle paths based on his knowledge of the design, although recently attempts have been made to automatically extract these paths from the RTL designs [86]. Finally, the design constraints may include physical location constraints, which specify that certain logic elements or blocks be placed at certain locations or a range of locations. These location constraints may be specified by the designer, or inherited from the previous design iteration (for making incremental changes), or generated automatically by the physical synthesis tools in the previous design iterations. We shall discuss the physical synthesis concept and techniques in Section 4.

- The third design input component is the choice of FPGA device. Each FPGA vendor typically provides a wide range of FPGA devices, with different performance, cost, and power tradeoffs. The selection of target device may be an iterative process. The designer may start with a small (low capacity) device with a nominal speed-grade. But, if synthesis effort fails to map the design into the target device, the designer has to upgrade to a high-capacity device. Similarly, if the synthesis result fails to meet the operating frequency, he has to upgrade to a device with higher speed-grade. In both the cases, the cost of the FPGA device will increase—in some cases by 50% or even by 100%. This clearly underscores the need to have better synthesis tools, since their quality directly impacts the performance and cost of FPGA designs.

We now briefly describe each step in the design flow shown in Fig. 1.6 and, following that, we present an outline of the remainder of this paper. Given an RTL design, a set of design constraints, and the target FPGA device, the overall FPGA synthesis process goes through the following steps:

- RTL elaboration. This identifies and/or infers *datapath* operations, such as additions, multiplications, register files, and/or memory blocks, and *control logic*, which is elaborated into a set of finite-state machines and/or generic Boolean

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networks. It is important to recognize the datapath elements as most of them have special architectural support in modern FPGAs, such as adders with dedicated fast-carry chains and embedded multipliers.

- Architecture-independent optimization. This includes both *datapath optimization*, using techniques such as constant propagation, strength reduction, operation sharing, and expression optimization; and *control logic optimization*, which includes both sequential optimization, such as finite-state machine encoding/minimization and retiming, and combinational logic optimization, such as constant propagation, redundancy removal, logic network restructuring and optimization, and don't-care based optimization.
- Technology mapping and architecture-specific optimization. This maps: (i) the optimized datapath to on-chip dedicated circuit structures, such as on-chip multipliers, adders with dedicated carry-chains, and embedded memory blocks for datapath implementation, and (ii) the optimized control logic to BLEs. Note that datapath operations can be mapped to BLEs as well if the dedicated circuit structures are not available or not convenient to use.
- Clustering and placement. Placement determines the location of each element in the mapped netlist. Since most modern FPGAs are hierarchical, a separate clustering step may be performed prior to placement to group BLEs into logic blocks. Alternatively, such clustering or grouping may be carried out during the placement process.
- Placement-driven optimization and incremental placement. Once placement is available, interconnects are defined and may become a performance bottleneck (since the delay of a long interconnect can be multiples of a BLE's delay). Further optimization may be carried out in the presence of interconnect delays, including logic restructuring, duplication, rewiring, etc. After such operations, an incremental placement step is needed to legalize the placement again.

The step of placement-driven optimization is optional, but may improve design performance considerably.

- Routing. Global routing and detail routing will be performed to connect all signal paths using the available programmable interconnects on-chip.
- Bit-stream generation. This is the final step of the design flow. It takes the mapped, placed, and routed design as input and generates the necessary bit-stream to program the logic and interconnects to implement the intended logic design and layout on the target FPGA device.

Following sections present the algorithms and techniques used in these steps in reverse order of the design flow. We start with routing and placement (Section 2), then present techniques used in technology mapping and architecture-specific optimization (Section 3). The architecture-dependent optimization phase of FPGA design typically shares techniques widely used for ASIC synthesis and optimization, and we refer the reader to the available textbooks [79, 98] for details. Section 4 presents the techniques used in physical synthesis of FPGA designs, which cover the algorithms used in clustering and placement-driven optimization. Section 5 presents the techniques used in RT-level and behavior-level synthesis for FPGA designs. Section 6 discusses synthesis techniques used for FPGA power optimization, which is a design objective that has received a lot of interest in recent years. This design objective cuts cross all design steps in the flow and interacts with performance and area optimization. Finally, we conclude this paper and touch on future trends of FPGA design automation in Section 7.

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