
**Discrete Circuit
Optimization:
Library Based
Gate Sizing and
Threshold Voltage
Assignment**

Discrete Circuit Optimization: Library Based Gate Sizing and Threshold Voltage Assignment

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Abstract

Discrete gate sizing and threshold assignment are commonly used tools for optimizing digital circuits, and ideal methods for incremental optimization. The gate widths and threshold voltages, along with the gate lengths, can be adjusted to optimize power and delay. This monograph surveys this field, providing the background needed to perform research in the field. Concepts such as standard cell libraries, static timing analysis, and analytical delay and power models are explained, along with examples and data to help understand the tradeoffs involved. Comparative results are also provided to show the current state of the field.

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Introduction

Gate sizing and threshold voltage assignment¹ are widely used to optimize digital circuits. They can be used to manage trade-offs in power, timing, area, yield, crosstalk, statistical power, statistical delay and soft-errors. They can also be used incrementally and as a method for optimizing post-layout designs after placement and interconnect routing. After over three decades, research is still active in the area.

This work will consider the case of gate sizing and threshold voltage assignment for standard library cell designs. In this context, gates are chosen from a library of pre-characterized gates that act as the fundamental building blocks. Cell-based designs compose the majority of the digital designs today.

1.1 Other Types of Cell Optimization Problems

There are other variants of gate sizing and threshold voltage assignment that are not covered in this work:

- (1) Transistor sizing for analog design
- (2) Transistor sizing for custom digital design

¹ While the title explicitly states the gate sizing and V_t assignment, the material is relevant to other cell optimization methods, such as gate-length biasing problems.

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These variants are a minority of IC designs. Custom digital design is mainly limited to high-performance designs. However, analog designs are becoming increasingly important with the increase in systems on a chip (SoC) methodologies that integrate entire TVs or radios on a single die [63].

1.1.1 Transistor Sizing for Analog Designs

In analog design, there are many different constraints and performance specifications: gain, accuracy, linearity, signal-to-noise, and impedance matching. For example, the pair of transistors forming a current mirror or differential pair must be *matched*, or have very similar electrical characteristics. Also, transistors that function as voltage-controlled resistors must be operating in the linear region, and an amplifier must have the proper signal-to-noise ratio for the system to work properly. While standard cells mask much of the underlying electrical waveforms using logic states, analog designs utilize these underlying characteristics to produce amplifiers, digital-to-analog converters, current sources, etc. However, many more facets of the design must be controlled for a proper function.

The main challenge in automated analog sizing is to input the design specifications and models into a form that can be used by the sizing method. This is challenging because the range of analog designs is large. For instance, while the analytical performance models for a given op-amp topology might be well known, it is difficult to write down the equations that govern the sizing of an *arbitrary* design.

Early methods for automated sizing were *knowledge-based*, where templates [52, 55, 72] were used to synthesize designs. These pre-characterized templates would carry information on a good initial sizing and on how to optimize the given template. Sizing these designs was therefore equivalent to executing the design plans. For example, in [52], the sizing proceeds by determining the bias current, then the W/L ratios, followed by the $1/f$ noise consideration, and finally the W and L of each device. In [72], the values are chosen using a fixed point method, where the parameters are determined serially. Each parameter is chosen to best satisfy the design considerations, assuming the other parameters to be fixed.

The time required to construct these templates, however, was often much greater than the time needed to design the circuit directly [63]. The accumulation of knowledge bases, and the codification of the expert knowledge was not practical. This, coupled with the limited range of circuits that the method could handle, led to the decline of these types of methods. However, there is recent interest in automating the knowledge-extraction process [108], and in identifying substructures in a design automatically [107].

Another branch of analog sizing is the *optimization-based* methods. These methods use optimization procedures, rather than codified design rules, to size the design. The first subclass of optimization methods consists of *equation based methods*² [64, 75, 87] that rely on the designer to provide the equations, but in contrast to the knowledge-based methods, the sizing process is automated using optimization methods, rather than rules. The optimization process may use simulated annealing [64], steepest-descent [87], or convex optimization [75]. This sub-class works well in certain contexts (such as in [75]), but they may be limited by their accuracy.

The second subclass of optimization based methods are the *simulation based methods* [54, 58, 88, 118, 119, 126] that use numerical simulations to measure the performance. The simulations provide these methods with greater accuracy, however they create a large overhead that makes these methods much slower than their equation-based counterparts.

1.1.2 Transistor Sizing for Custom Digital Designs

In the custom digital setting, every transistor in the design is available for optimization [7, 44, 45, 82, 153]. The early papers on gate sizing were based on transistor-level sizing (see [60, 135]), until standard cells became widespread in the 1990s.³ With the increasing complexity of designs, standard cell libraries are almost universally used.

Custom digital design techniques are primarily used for high-performance parts of high-volume designs which is needed to recover

² See [63] for the taxonomy of analog sizing methods and a comprehensive review of methods prior to 2000.

³ See, for example, [159].

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the increased cost of designing at a transistor level, as in the case of microprocessors [12]. Custom digital transistor sizing is still an active area of research today and most current research is directed toward the statistical design of custom circuits [8, 43, 146]. However, these methods account for a minority of the digital designs.

1.2 The Physical Design Process

Gate sizing and threshold voltage assignment are a part of the larger Electronic Design Automation (EDA) ecosystem that transforms Register Transfer Language (RTL) descriptions into a physical layout. The process of creating the physical layout is called the *physical design* process, and consists of six steps:

(1) Logic synthesis.

- Input: RTL/HDL design description, standard cell library information, timing constraint information.
- Output: Netlist mapped to the standard cell library.

Transform the RTL/HDL design description into a gate level netlist, using a given cell library. Convert state machines, map arithmetic blocks, etc.

(2) Floorplanning.

- Input: synthesized netlist, macro information, standard cell library information, standard cell row information, information on chip inputs and outputs.
- Output: floorplan with rows for standard cell placement, pads for input and output, locations for macros.

Create a die for the design, and allocate space for input–output ports, macros, and library gates.

(3) Placement.

- Input: synthesized netlist, floorplan.
- Output: locations for each of the cells in the design in a standard cell row.

Places, flips and rotates cells into the rows created by the floorplanning algorithm. Minimizes the wirelength in the resulting layout, while meeting timing constraints (timing-driven placement).

(4) **Clock Tree synthesis.**

- Input: placed design, clock nets.
- Output: clock tree to distribute the clock signal to the sequential elements (flip-flops, latches, etc.).

Creates a clock tree to distribute the clock signal across the design. The goals are to minimize the size of the clock tree (to minimize power), and the skew at each of the outputs of the clock tree. Buffers may be added to help distribute the clock signal.

(5) **Routing.**

- Input: placed design, connection information, metal and via information from the library.
- Output: design with cells connected with wires.

Connects cells in the library using metal layers and vias. The objective is to minimize the amount of interconnect needed, while observing design rules and meeting timing.

(6) **Physical verification and yield enhancement.**

- Input: placed, routed design.
- Output: verified design with improved yield.

Improves the yield of the design. Corrects design rules violations, inserts metal fill, doubles vias, checks connectivity and topology.

A flowchart for the EDA process is shown in Figure 1.1.

Although gate sizing and threshold voltage assignment are not explicitly in the design flow above, they are used throughout the design flow to correct timing errors, and to optimize the design. For example, they are commonly used after placement to resize gates that violate maximum fanout rules or flip-flop setup time requirements (see, for example [22]). After clock tree synthesis, they are used to further fix

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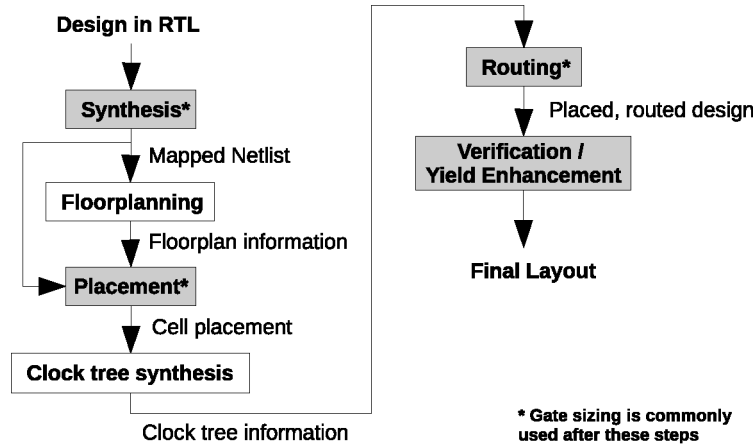


Fig. 1.1 Electronic Design Automation flow.

rule violations and setup and hold violations, using the clock information from the clock-tree synthesis. After routing, they are again used to fix setup and hold violations, along with design rule violations. At this step, an incremental routing may be needed to account for changes in the cell sizes, and their corresponding pin locations.

They are also used at different points in the design flow to reduce the power consumption [2]. While this may reduce the power *using the same timing constraint*, in other instances the timing constraints may need to be relaxed to achieve a power reduction.

Gate sizing and threshold voltage assignment are powerful tools for optimization, and are the most widely used incremental optimization tools. These methods are more powerful and less intrusive than adjusting the placement or routing of the design. For example, fixing setup time violations using placement would require the gates on the violating path to be moved, and would require rerouting the interconnects. Similarly, fixing setup time violations using routing would also require the connections between the cells to be rerouted. In both the cases, a significant portion of the design will need to be rerouted to provide benefits.

On the other hand, gate sizing and threshold voltage assignment are less disruptive than re-placing the cells or re-routing them. For example, the timing of a buffer driving a large wire load could be improved

by increasing its size. This may result in a local rerouting to accommodate the different pin locations of the larger cell, and if there is no space around the surrounding cell, then an incremental placement will be needed to create space for the cell. However, this is preferable to rerouting large sections of the design, or adjusting the placements of tens or hundreds of cells.

In some cases, when only the gate lengths or threshold voltages change, the disruption is very minimal. In these cases, the cell dimensions and pin locations are the same, and these cell alternatives can be swapped without any change in the routing or the placement. The only verification needed is to ensure that the crosstalk noise, power, and timing constraints are satisfied.

Another advantage of gate sizing and threshold voltage assignment is that they are *versatile*, as they can be targeted to different optimization objectives. They have been used for power and timing optimization [46], to fix noise constraints due to crosstalk [98, 170], to harden soft-errors due to radiation [174], to improve yield [37, 50], and to minimize statistical power [42, 151].

1.3 The Standard Cell Library

The standard cell library contains logic cells such as inverters, ands, not-and (nands), and x-ors that implement Boolean logic functions. There are also sets of sequential cells such as flip-flops, latches, and their variants with capabilities for setting, resetting and reading in scan-chains. These sequential cells provide *memory*, allowing pipe-lining, state machines, and a memory for computations. Lastly, there are utility cells, such as filler cells, antenna cells, and buffer cells, which are tools to help with the physical implementation of the design.

The library generally provides several gate options for each logic function. Each of the options are logically equivalent — they implement the same boolean function — but have varying electrical characteristics, due to differences in their gate lengths, widths, PMOS–NMOS width ratios and threshold voltages V_t . These alternative options can be used to optimize the design. For example, critical paths can be sped up by swapping high- V_t cells by low- V_t cells, and gates with fanout violations

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can be fixed using alternatives with larger-transistor widths and smaller effective resistances at the gate outputs.

Two library files that are used for sizing and threshold voltage assignment are:

(1) **Physical library information.**

(usually expressed in Library Exchange Format (LEF)):

- Cell information: dimensions of the cell and locations of the pins.
- Interconnect information: dimensions, pitch, capacitance, and resistances for each metal layer.
- Via information: dimensions, resistance, and layers that are connected.

(2) **Timing library information.**

(usually expressed in Liberty Format):

- Library characterization information: temperature, voltage and process.
- Parameters used in the library: slew thresholds, input thresholds, output thresholds, and measurement units.
- Cell information: delays, area, logic function, short-circuit power, switching power, leakage power. For flip-flops the hold and setup time requirements are also given.
- Cell pin information: capacitances, maximum loads.

The geometry information in the LEF file is used for placement and routing. This information tells the program how to create standard cell rows for floorplanning, and the dimensions of each cell for placement. Next, the pin locations, interconnect geometries, and via dimensions are used for routing, and once routing is complete, the capacitance and resistance information is used to extract information about the wire parasitics.

The timing and power information from the Liberty file is used for the timing and power analysis of the design. The timing information

is used in conjunction with the wire parasitic information to create delay estimates and power estimates with interconnect loading modeling. This will be covered in more detail in Section 2.4.

1.4 The Gate Sizing and V_t Assignment Problem

Of the many variations on the gate sizing and threshold voltage assignment problem, this work will consider the following metrics:

- Leakage power
- Dynamic power
- Clock period

The application most commonly found in literature today is to minimize the power, or some combination of the leakage power and the dynamic power, with a constraint on the clock period. When timing closure is important, the objective is to minimize the clock period, and in post-layout situations, the noise and crosstalk violations are often optimized.

The variables in the optimization process are the cells used to implement the gates. These cells can be swapped to decrease the delay or power, or to modify the output signal waveform. The cells may be different sizes, and have different pin locations.

Functionally equivalent cells that can be interchanged may be identified by the designer, the design tool, or by the library by having the same *footprint*. For example, the inverter-type cells will have an “inverter” footprint, which identifies the family of cells that can be used to replace the gate. Each of these cells performs the same logic function, thus changing the cells does not affect the functionality of the design.

Formally, the problem may be written as an optimization problem. For example, with the vector of cell options $\vec{\omega}$, the delay-constrained power optimization problem is:

$$\begin{aligned} & \text{minimize} && \text{Power}(\vec{\omega}) \\ & \text{subject to} && \text{Delay}(\vec{\omega}) \leq T_{\max} \end{aligned} \tag{1.1}$$

where T_{\max} is the clock period. This form helps summarize the objectives and constraints in the optimization process.

Table 1.1. Notation.

Symbol	Meaning
\mathcal{G}	Set of gates in the design
g	A gate in the design
ω, ω_0	A cell option, current cell option
CellOptions(g)	Set of alternative library cell options for g
w_g	The width for gate g
v_{th_g}	The threshold voltage for gate g
t_a	Arrival time
$t_{a(g)}$	Set of arrival times for the inputs of gate g
t_r	Required arrival time
$t_{r(g)}$	Set of required arrival times for the inputs of gate g
τ_g	Set of input transition slews for gate g
d	Delay
p	Power
PI	<i>Primary inputs</i> input ports in the design
PO	<i>Output ports</i> in the design
fi(g)	The set of gates that drive the inputs of gate g
fo(g)	The set of gates that are connected to the output of gate g
ϵ	A small positive number
ρ	Power/delay tradeoff sensitivity

The delay is estimated using a Static Timing Analysis method (see Section 2) and timing constraints are usually expressed in a Synopsys Design Constraint (SDC) format. These constraints can be very complex, with multicycle paths, multiple clocks, power domains, and false-path definitions. In addition, parasitic information in a Standard Parasitic Exchange (SPEF) format is used to approximate the interconnect delay.

1.5 Notations and Acronyms

While new notation is avoided when possible, notation for certain key concepts are unavoidable. The notation for key symbols used in this monograph are summarized in Table 1.1. These symbols, and concepts, will be elaborated in the remainder of the monograph; for example, the slew and other timing concepts will be covered in the following section.

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